Introduction

LinkSwitch-TN combines a high voltage power MOSFET switch with an ON/OFF controller in one device. It is completely self-powered from the DRAIN pin, has a jittered switching frequency for low EMI and is fully fault protected. Auto-restart limits device and circuit dissipation during overload and output short circuit (LNK304-306) while over temperature protection disables the internal MOSFET during thermal faults. The high thermal shutdown threshold is ideal for applications where the ambient temperature is high while the large hysteresis protects the PCB and surrounding components from high average temperatures.

LinkSwitch-TN is designed for any application where a non-isolated supply is required such as appliances (coffee machines, rice cookers, dishwashers, microwave ovens etc.), night lights, emergency exit signs and LED drivers. LinkSwitch-TN can be configured in all common topologies to give a line or neutral referenced output and an inverted or non-inverted output voltage – ideal for applications using TRIACs for AC load control. Using a switching power supply rather than a passive dropper (capacitive or resistive) gives a number of advantages, some of which are listed below.

- Universal input – the same power supply/product can be used worldwide
- High power density – smaller size, no µF's of X class capacitance needed
- High efficiency – full load efficiencies >75% typical for 12 V output
- Excellent line and load regulation
- High efficiency at light load – ON/OFF control maintains high efficiency even at light load
- Extremely energy efficient – input power <100 mW at no load
- Entirely manufacturable in SMD
- More robust to drop test mechanical shock
- Fully fault protected (overload, short circuit and thermal faults)
- Scalable – LinkSwitch-TN family allows the same basic design to be used from <50 mA to 360 mA

Scope

This application note is for engineers designing a non-isolated power supply using the LinkSwitch-TN family of devices. This document describes the design procedure for buck and buck-boost converters using the LinkSwitch-TN family of integrated off-line switchers. The objective of this document is to provide power supply engineers with guidelines in order to enable them to quickly build efficient and low cost buck or buck-boost converter based power supplies using low cost off-the-shelf inductors. Complete design equations are provided for the selection of the converter’s key components. Since the power MOSFET and controller are integrated into a single IC the design process is greatly simplified, the circuit configuration has few parts and no transformer is required. Therefore a quick start section is provided that allows off-the-shelf components to be selected for common output voltages and currents.

Figure 1(a). Basic Configuration Using LinkSwitch-TN in a Buck Converter. Figure 1(b). Basic Configuration Using LinkSwitch-TN in a Buck-Boost Converter.

www.powerint.com
March 2014
In addition to this application note a design spreadsheet is available within the PIXls tool in the PI Expert design software suite. The reader may also find the LinkSwitch-TN DAK engineering prototype board useful as an example of a working supply. Further details of support tools and updates to this document can be found at www.powerint.com.

Quick Start

Readers wanting to start immediately can use the following information to quickly select the components for a new design, using Figure 1 and Tables 1 and 2 as references.

1. For AC input designs select the input stage (Table 9).
2. Select the topology (Tables 1 and 2). If better than ±10% output regulation is required, then use optocoupler feedback with suitable reference.
3. Select the LinkSwitch-TN device, \( L, R_{\text{FB}} \) or \( V_z, R_{\text{Z}} \), \( C_{\text{FB}} \), \( R_{\text{Z}} \) and the reverse recovery time for \( D_{\text{FW}} \) (Table 4: Buck, Table 5: Buck-Boost).
4. Select freewheeling diode to meet \( t_r \) determined in Step 3 (Table 3).
5. For direct feedback designs, if the minimum load <3 mA then calculate \( R_{\text{PL}} = \frac{V_o}{3 \text{ mA}} \).
6. Select \( C_o \) as 100 \( \mu \text{F}, 1.25 \times V_{o}, \) low ESR type.
7. Construct prototype and verify design.

<table>
<thead>
<tr>
<th>Topology</th>
<th>Basic Circuit Schematic</th>
<th>Key Features</th>
</tr>
</thead>
</table>
| High-Side Buck – Direct Feedback | ![Basic Circuit Schematic](topology1.png) | 1. Output referenced to input.  
2. Positive output (\( V_o \)) with respect to \(-V_{n} \).  
3. Step down – \( V_o < V_{n} \).  
4. Low cost direct feedback (±10% typ.).  
5. Requires an output load to maintain regulation (Note 2). |
| High-Side Buck-Boost – Direct Feedback | ![Basic Circuit Schematic](topology2.png) | 1. Output referenced to input.  
2. Negative output (\( V_o \)) with respect to \(-V_{n} \).  
3. Step down – \( V_o > V_{n} \) or \( V_o < V_{n} \).  
4. Low cost direct feedback (±10% typ.).  
5. Fail-safe – output is not subjected to input voltage if the internal MOSFET fails.  
6. Ideal for driving LEDs – better accuracy and temperature stability than low-side buck constant current LED driver.  
7. Requires an output load to maintain regulation (Note 2). |

Notes:
1. Low Cost, directly sensed feedback typically achieves overall regulation tolerance of ±10%.
2. To ensure output regulation, a pre-load may be required to maintain a minimum load current of 3 mA (buck and buck-boost only).
3. Boost topology (step up) also possible but not shown.

Table 1. LinkSwitch-TN Circuit Configurations Using Directly Sensed Feedback.
Topology | Basic Circuit Schematic | Key Features
--- | --- | ---
High-Side Buck – Optocoupler Feedback | ![High-Side Buck – Optocoupler Feedback Circuit](PI-3706-A1779) | 1. Output referenced to input.  
2. Positive output \( V_O \) with respect to \(-V_{IN} \).  
3. Step down – \( V_O < V_{IN} \).  
4. Optocoupler feedback.  
- Accuracy only limited by reference choice  
- Low cost non-safety rated optocoupler  
- No pre-load required  
5. Minimum no-load consumption.

Low-Side Buck – Optocoupler Feedback | ![Low-Side Buck – Optocoupler Feedback Circuit](PI-3707-A1779) | 1. Output referenced to input.  
2. Negative output \( V_O \) with respect to \(+V_{IN} \).  
3. Step down – \( V_O < V_{IN} \).  
4. Optocoupler feedback.  
- Accuracy only limited by reference choice  
- Low cost non-safety rated optocoupler  
- No pre-load required

Low-Side Buck-Boost – Optocoupler Feedback | ![Low-Side Buck-Boost – Optocoupler Feedback Circuit](PI-3708-A1779) | 1. Output referenced to input.  
2. Positive output \( V_O \) with respect to \(+V_{IN} \).  
3. Step up/down – \( V_O > V_{IN} \) or \( V_O < V_{IN} \).  
4. Optocoupler feedback.  
- Accuracy only limited by reference choice  
- Low cost non-safety rated optocoupler  
- No pre-load required  
5. Fail-safe – output is not subjected to input voltage if the internal MOSFET fails.  

Notes:
1. Performance of opto feedback only limited by accuracy of reference (Zener or IC).  
2. Optocoupler does not need to be safety approved.  
3. Reference bias current provides minimum load. The value of \( R_Z \) is determined by Zener test current or reference IC bias current, typically 470 \( \Omega \) to 2 k\( \Omega \), 1/8 W, 5%.  
4. Boost topology (step-up) is also possible but not shown.  
5. Optocoupler feedback provides lowest no-load consumption.

Table 2. LinkSwitch-TN Circuit Configurations Using Optocoupler Feedback.

<table>
<thead>
<tr>
<th>Part Number</th>
<th>( V_{RRM} ) (V)</th>
<th>( I_F ) (A)</th>
<th>( t_{rr} ) (ns)</th>
<th>Package</th>
<th>Manufacturer</th>
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Table 3. List of Ultrafast Diodes Suitable for use as the Freewheeling Diode.
### Table 4. Components Quick Select for Buck Converters.

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<th>V&lt;sub&gt;OUT&lt;/sub&gt;</th>
<th>I&lt;sub&gt;OUT(MAX)&lt;/sub&gt;</th>
<th>Inductor</th>
<th>LNK30X</th>
<th>Mode</th>
<th>Diode</th>
<th>t&lt;sub&gt;rr&lt;/sub&gt;</th>
<th>R&lt;sub&gt;FB&lt;/sub&gt;</th>
<th>V&lt;sub&gt;Z&lt;/sub&gt;</th>
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Other Standard Components

- **R<sub>BIAS</sub>**: 2 kΩ, 1%, 1/8 W
- **C<sub>BF</sub>**: 0.1 μF, 50 V Ceramic
- **C<sub>FB</sub>**: 10 μF, 1.25 × V<sub>OUT</sub>
- **D<sub>FB</sub>**: 1N4005GP
- **R<sub>Z</sub>**: 470 Ω to 2 kΩ, 1/8 W, 5%

*Select nearest standard or combination of standard values.*
### Table 5. Components Quick Select for Buck-Boost Converters.  *Select nearest standard or combination of standard values.

<table>
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<th>$V_{OUT}$</th>
<th>$I_{OUT(\text{MAX})}$</th>
<th>Inductor</th>
<th>$\mu H$</th>
<th>$I_{\text{RMS}}$ (mA)</th>
<th>LNK30X</th>
<th>Mode</th>
<th>Diode $t_{tr}$</th>
<th>$R_{FB}$ *</th>
<th>$V_Z$</th>
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<td>5</td>
<td>85</td>
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<td>220</td>
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<td>340</td>
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<td>3000</td>
<td>90</td>
<td>SBC3-332-151</td>
<td>RFB0807-222 RFB0807-332</td>
<td>≤ 75 ns</td>
</tr>
<tr>
<td></td>
<td>85</td>
<td>2200</td>
<td>70</td>
<td>85</td>
<td>180</td>
<td>-</td>
<td>SBC3-222-191</td>
<td>RFB0807-222 RFB0807-332</td>
<td>≤ 75 ns</td>
</tr>
<tr>
<td></td>
<td>120</td>
<td>1200</td>
<td>220</td>
<td>120</td>
<td>220</td>
<td>-</td>
<td>SBC3-332-151</td>
<td>RFB0807-222 RFB0807-332</td>
<td>≤ 75 ns</td>
</tr>
<tr>
<td></td>
<td>160</td>
<td>1600</td>
<td>220</td>
<td>160</td>
<td>210</td>
<td>-</td>
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<td>≤ 75 ns</td>
</tr>
<tr>
<td></td>
<td>175</td>
<td>820</td>
<td>320</td>
<td>225</td>
<td>320</td>
<td>-</td>
<td>SBC4-681-431</td>
<td>RFB0807-821 RFB0810-122</td>
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</tr>
<tr>
<td></td>
<td>280</td>
<td>820</td>
<td>410</td>
<td>360</td>
<td>410</td>
<td>-</td>
<td>SBC4-681-431</td>
<td>RFB0807-821 RFB0810-122</td>
<td>≤ 75 ns</td>
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<td></td>
<td>≤65</td>
<td>2200</td>
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<td>680</td>
<td>100</td>
<td>SBC3-332-151</td>
<td>RFB0807-821 RFB0810-122</td>
<td>≤ 75 ns</td>
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<td></td>
<td>70</td>
<td>2200</td>
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<td>180</td>
<td>-</td>
<td>SBC3-332-151</td>
<td>RFB0807-821 RFB0810-122</td>
<td>≤ 75 ns</td>
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<td></td>
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<td>680</td>
<td>180</td>
<td>160</td>
<td>220</td>
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<td>SBC3-332-151</td>
<td>RFB0807-821 RFB0810-122</td>
<td>≤ 75 ns</td>
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<td>SBC4-681-431</td>
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<td>410</td>
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<td>SBC4-681-431</td>
<td>RFB0807-821 RFB0810-122</td>
<td>≤ 75 ns</td>
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<td></td>
<td>≤65</td>
<td>3300</td>
<td>70</td>
<td>80</td>
<td>3300</td>
<td>100</td>
<td>SBC3-682-111</td>
<td>RFB0807-332 RFB0807-682</td>
<td>≤ 75 ns</td>
</tr>
<tr>
<td></td>
<td>70</td>
<td>680</td>
<td>180</td>
<td>120</td>
<td>210</td>
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<td>SBC3-682-111</td>
<td>RFB0807-332 RFB0807-682</td>
<td>≤ 75 ns</td>
</tr>
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<td></td>
<td>15</td>
<td>3300</td>
<td>70</td>
<td>160</td>
<td>3300</td>
<td>100</td>
<td>SBC3-682-111</td>
<td>RFB0807-332 RFB0807-682</td>
<td>≤ 75 ns</td>
</tr>
<tr>
<td>24</td>
<td>50</td>
<td>1800</td>
<td>300</td>
<td>225</td>
<td>200</td>
<td>-</td>
<td>SBC4-681-431</td>
<td>RFB0810-182 RFB1010-222</td>
<td>≤ 75 ns</td>
</tr>
<tr>
<td></td>
<td>175</td>
<td>1800</td>
<td>300</td>
<td>225</td>
<td>290</td>
<td>-</td>
<td>SBC4-681-431</td>
<td>RFB0810-182 RFB1010-222</td>
<td>≤ 75 ns</td>
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<tr>
<td></td>
<td>280</td>
<td>1800</td>
<td>370</td>
<td>360</td>
<td>410</td>
<td>-</td>
<td>SBC4-681-431</td>
<td>RFB0810-182 RFB1010-222</td>
<td>≤ 75 ns</td>
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<tr>
<td></td>
<td>≤65</td>
<td>3300</td>
<td>70</td>
<td>80</td>
<td>3300</td>
<td>100</td>
<td>SBC3-682-111</td>
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<td></td>
<td>70</td>
<td>680</td>
<td>180</td>
<td>120</td>
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<td>-</td>
<td>SBC3-682-111</td>
<td>RFB0810-182 RFB1010-222</td>
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</tr>
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<td>300</td>
<td>160</td>
<td>3300</td>
<td>100</td>
<td>SBC3-682-111</td>
<td>RFB0810-182 RFB1010-222</td>
<td>≤ 75 ns</td>
</tr>
</tbody>
</table>

Other Standard Components

$R_{BIAS}$: 2 kΩ, 1%, 1/8 W

$C_{BP}$: 0.1 μF, 50 V Ceramic

$C_{FB}$: 10 μF, 1.25 × $V_O$

$D_{FB}$: 1N4005GP

$R_Z$: 470 Ω to 2 kΩ, 1/8 W, 5%

*Select nearest standard or combination of standard values.
LinkSwitch-TN Circuit Design

LinkSwitch-TN Operation

The basic circuit configuration for a buck converter using LinkSwitch-TN is shown in Figure 1(a).

To regulate the output, an ON/OFF control scheme is used as illustrated in Table 6. As the decision to switch is made on a cycle-by-cycle basis, the resultant power supply has extremely good transient response and removes the need for control loop compensation components. If no feedback is received for 50 ms, then the supply enters auto-restart (LNK304-306 only).

Reference Schematic And Key

<table>
<thead>
<tr>
<th>Reference Schematic And Key</th>
</tr>
</thead>
<tbody>
<tr>
<td><img src="image1.png" alt="Reference Schematic And Key" /></td>
</tr>
</tbody>
</table>

Normal Operation

At the beginning of each cycle, the FEEDBACK (FB) pin is sampled.
- If \( I_{FB} < 49 \, \mu A \) then next cycle occurs
- If \( I_{FB} > 49 \, \mu A \) then next switching cycle is skipped

High load – few cycles skipped

Low load – many cycles skipped

Auto-Restart (LNK304-306 only)

If no feedback \( I_{FB} < 49 \, \mu A \) for > 50 ms, then output switching is disabled for approximately 800 ms.

Table 6. LinkSwitch-TN Operation.
To allow direct sensing of the output voltage without the need for a reference (Zener diode or reference IC), the FEEDBACK pin voltage is tightly tolerated over the entire operating temperature range. For example, this allows a 12 V design with an overall output tolerance of ±10%. For higher performance, an opto-coupler can be used with a reference as shown in Table 2. Since the optocoupler just provides level shifting, it does not need to be safety rated or approved. The use of an opto-coupler also allows flexibility in the location of the device, for example it allows a buck converter configuration with the LinkSwitch-TN in the low-side return rail, reducing EMI as the SOURCE pins and connected components are no longer part of the switching node.

Selecting the Topology

If possible, use the buck topology. The buck topology maximizes the available output power from a given LinkSwitch-TN and inductor value. Also, the voltage stress on the power switch and freewheeling diode and the average current through the output inductor are slightly lower in the buck topology as compared to the buck-boost topology.

Selecting the Operating Mode – MDCM and CCM Operation

At the start of a design, select between mostly discontinuous conduction mode (MDCM) and continuous conduction mode (CCM) as this decides the selection of the LinkSwitch-TN device, freewheeling diode and inductor. For maximum output current select CCM, for all other cases MDCM is recommended. Over-all, select the operating mode and components to give the lowest overall solution cost. Table 7 summarizes the trade-offs between the two operating modes.

Additional differences between CCM and MDCM include better transient response for DCM and lower output ripple (for same capacitor ESR) for CCM. However these differences, at the low

<table>
<thead>
<tr>
<th>Operating Mode</th>
<th>MDCM</th>
<th>CCM</th>
</tr>
</thead>
<tbody>
<tr>
<td>Operating Description</td>
<td><img src="pi-3769-121803" alt="Inductor current falls to zero during t_{OFF}, borderline between MDCM and CCM when t_{IDLE} = 0." /></td>
<td><img src="pi-3770-121503" alt="Current flows continuously in the inductor for the entire duration of a switching cycle." /></td>
</tr>
<tr>
<td>Inductor</td>
<td>Lower Cost Lower value, smaller size.</td>
<td>Higher Cost Higher value, larger size.</td>
</tr>
<tr>
<td>Freewheeling Diode</td>
<td>Lower Cost 75 ns ultrafast reverse recovery type (≤35 ns for ambient &gt;70 °C).</td>
<td>Higher Cost 35 ns ultrafast recovery type required.</td>
</tr>
<tr>
<td>LinkSwitch-TN</td>
<td>Potentially Higher Cost May require larger device to deliver required output current–depends on required output current.</td>
<td>Potentially Lowest Cost May allow smaller device to deliver required output current–depends on required output current.</td>
</tr>
<tr>
<td>Overall</td>
<td></td>
<td>Typically Higher Cost</td>
</tr>
</tbody>
</table>

Table 7: Comparison of Mostly Discontinuous Conduction (MDCM) and Continuous Conduction (CCM) Modes of Operation.
output currents of LinkSwitch-TN applications, are normally not significant.

The conduction mode CCM or MDCM of a buck or buck-boost converter primarily depends on input voltage, output voltage, output current and device current limit. The input voltage, output voltage and output current are fixed design parameters, therefore the LinkSwitch-TN (current limit) is the only design parameter that sets the conduction mode.

The phrase "mostly discontinuous" is used as with On/Off control, since a few switching cycles may exhibit continuous inductor current, the majority of the switching cycles will be in the discontinuous conduction mode. A design can be made fully discontinuous but that will limit the available output current, making the design less cost effective.

**Step-by-Step Design Procedure**

**Step 1. Determine System Requirements VAC\textsubscript{MIN}, VAC\textsubscript{MAX}, P\textsubscript{O}, V\textsubscript{O}, f\textsubscript{L}, \eta**

Determine the input voltage range from Table 8.

<table>
<thead>
<tr>
<th>Input (VAC)</th>
<th>VAC\textsubscript{MIN}</th>
<th>VAC\textsubscript{MAX}</th>
</tr>
</thead>
<tbody>
<tr>
<td>100/115</td>
<td>85</td>
<td>132</td>
</tr>
<tr>
<td>230</td>
<td>195</td>
<td>265</td>
</tr>
<tr>
<td>Universal</td>
<td>85</td>
<td>265</td>
</tr>
</tbody>
</table>

*Table 8. Standard Worldwide Input Line Voltage Ranges.*

Line Frequency, f\textsubscript{l}: 50 or 60 Hz, for half-wave rectification use f\textsubscript{l}/2.

Output Voltage, V\textsubscript{O} in Volts.

Output Power, P\textsubscript{O} in Watts.

Power supply efficiency, \eta: 0.7 for a 12 V output, 0.55 for a 5 V output if no better reference data available.

<table>
<thead>
<tr>
<th>AC Input Voltage (VAC)</th>
<th>Total Capacitance C\textsubscript{TOTA\textsubscript{L}} (\mu\textsubscript{F}/P\textsubscript{OUT} (C\textsubscript{IN} + C\textsubscript{PAS}))</th>
</tr>
</thead>
<tbody>
<tr>
<td>100/115</td>
<td>6-8</td>
</tr>
<tr>
<td>230</td>
<td>1-2</td>
</tr>
<tr>
<td>Universal</td>
<td>6-8</td>
</tr>
</tbody>
</table>

*Table 10. Suggested Total Input Capacitance Values for Different Input Voltage Ranges.*

**Step 2. Determine AC Input Stage**

The input stage comprises fusible resistor(s), input rectification diodes and line filter network. The fusible resistor should be chosen as flameproof and, depending on the differential line input surge requirements, a wire-wound type may be required. The fusible resistor(s) provides fuse safety, inrush current limiting and differential mode noise attenuation.

For designs ≤1 W, it is lower cost to use half-wave rectification; >1 W, full wave rectification (smaller input capacitors). The EMI performance of half-wave rectified designs is improved by adding a second diode in the lower return rail. This provides EMI gating (EMI currents only flow when the diode is conducting) and also doubles differential surge withstand as the surge voltage is shared across two diodes. Table 9 shows the recommended input stage based on output power for a universal input design while Table 10 shows how to adjust the input capacitance for other input voltage ranges.

*Table 9. Recommended AC Input Stages for Universal Input.*
**Step 3. Determine Minimum and Maximum DC Input Voltages** \( V_{\text{MIN}} \) and \( V_{\text{MAX}} \) Based on AC Input Voltage

Calculate \( V_{\text{MAX}} \) as

\[
V_{\text{MAX}} = \sqrt{2} \times V_{\text{AXMAX}}
\]

Assuming that the value of input fusible resistor is small, the voltage drop across it can be ignored.

Assume bridge diode conduction time of \( t_c = 3 \text{ ms} \) if no other data available.

Derive minimum input voltage \( V_{\text{MIN}} \)

\[
V_{\text{MIN}} = \sqrt{2} \times \left( 2 \times V_{\text{ACMIN}}^3 - \frac{2 \times P_o \left( \frac{1}{2} \times f \right) - t_c}{\eta \times C_{\text{IN(TOTAL)}}} \right)
\]

If \( V_{\text{MIN}} \) is \( \leq 70 \text{ V} \) then increase value of \( C_{\text{IN(TOTAL)}} \).

**Step 4. Select LinkSwitch-TN Device Based on Output Current and Current Limit**

Decide on the operating mode - refer to Table 7.

For MDCM operation, the output current \( I_o \) should be less than or equal to half the value of the minimum current limit of the chosen device from the data sheet.

\[
I_{\text{LIMIT MIN}} \geq 2 \times I_o
\]

For CCM operation, the device should be chosen such that the output current \( I_o \) is more than 50%, but less than 80% of the minimum current limit \( I_{\text{LIMIT MIN}} \).

\[
0.5 \times I_{\text{LIMIT MIN}} < I_o < 0.8 \times I_{\text{LIMIT MIN}}
\]

Please see the data sheet for LinkSwitch-TN current limit values.

**Step 5. Select the Output Inductor**

Tables 4 and 5 provide inductor values and RMS current ratings for common output voltages and currents based on the calculations in the design spreadsheet. Select the next nearest higher voltage and/or current above the required output specification. Alternatively, the PI Expert software design suite or Appendix A can be used to calculate the exact inductor value (Eq. A7) and RMS current rating (Eq. A21).

It is recommended that the value of inductor chosen should be closer to \( L_{\text{TYP}} \) rather than \( 1.5 \times L_{\text{TYP}} \) due to lower DC resistance and higher RMS rating. The lower limit of 680 \( \mu \text{H} \) limits the maximum \( \frac{dI}{dt} \) to prevent very high peak current values. Tables 3 and 4 provide reference part numbers for standard inductors from two suppliers.

\[
680 \mu \text{H} < L_{\text{TYP}} < L < 1.5 \times L_{\text{TYP}}
\]

For LinkSwitch-TN designs, the mode of operation is not dependent on the inductor value. The mode of operation is a function of load current and current limit of the chosen device. The inductor value merely sets the average switching frequency.

Figure 2 shows a typical standard inductor manufacturer's data sheet. The value of off-the-shelf “drum core / dog bone / I core” inductors will drop up to 20% in value as the current increases. The constant \( K_{L\_\text{TOL}} \) in equation (A7) and the design spreadsheet adjusts for both this drop and the initial inductance value tolerance.

For example if a 680 \( \mu \text{H}, 360 \text{ mA} \) inductor is required, referring to Figure 2, the tolerance is 10% and an estimated 9.5% for the reduction in inductance at the operating current (approximately \([0.36/0.38] \times 10 \) ). Therefore the value of \( K_{L\_\text{TOL}} \) is 1.195 (19.5%). If no data is available, assume a \( K_{L\_\text{TOL}} \) of 1.15 (15%).

<table>
<thead>
<tr>
<th>Model</th>
<th>Inductance (L(mH/ at 10 kHz max.))</th>
<th>Rdc (µH)</th>
<th>Rated Current (A)</th>
<th>Current Rating for Value -10%</th>
</tr>
</thead>
<tbody>
<tr>
<td>681-361</td>
<td>680 10%</td>
<td>1.62</td>
<td>0.36</td>
<td>0.39</td>
</tr>
<tr>
<td>102-281</td>
<td>1000 10%</td>
<td>2.37</td>
<td>0.28</td>
<td>0.31</td>
</tr>
<tr>
<td>152-251</td>
<td>1500 10%</td>
<td>3.64</td>
<td>0.25</td>
<td>0.35</td>
</tr>
<tr>
<td>222-191</td>
<td>2200 10%</td>
<td>5.62</td>
<td>0.26</td>
<td>0.21</td>
</tr>
<tr>
<td>332-151</td>
<td>3300 10%</td>
<td>7.66</td>
<td>0.19</td>
<td>0.21</td>
</tr>
</tbody>
</table>

Figure 2. Example of Standard Inductor Data Sheet.
Not all the energy stored in the inductor is delivered to the load, due to losses in the inductor itself. To compensate for this, a loss factor $K_{\text{Loss}}$ is used. This has a recommended value of between 50% and 66% of the total supply losses as given by Equation 6. For example, a design with an overall efficiency ($\eta$) of 0.75 would have a $K_{\text{Loss}}$ value of between 0.875 and 0.833.

$$K_{\text{Loss}} = 1 - \left(1 - \frac{1 - \eta}{2}\right) = 1 - \left(\frac{2(1 - \eta)}{3}\right)$$  \hspace{1cm} (6)

**Step 6. Select Freewheeling Diode**

For MDCM operation at $t_{\text{AMB}} \leq 70 \degree C$, select an ultra-fast diode with $t_r \leq 75 \text{ ns}$. At $t_{\text{AMB}} > 70 \degree C$, $t_r \leq 35 \text{ ns}$. For CCM operation, select an ultra-fast diode with $t_r \leq 35 \text{ ns}$. Allowing 25% design margin for the freewheeling diode,

$$V_{\text{FIV}} > 1.25 \times V_{\text{MAX}}$$  \hspace{1cm} (7)

The diode must be able to conduct the full load current. Thus

$$I_F > 1.25 \times I_o$$  \hspace{1cm} (8)

Table 3 lists common freewheeling diode choices.

**Step 7. Select Output Capacitor**

The output capacitor should be chosen based on the output voltage ripple requirement. Typically the output voltage ripple is dominated by the capacitor ESR and can be estimated as:

$$\text{ESR}_{\text{MAX}} = \frac{V_{\text{RIPPLE}}}{\text{I}_{\text{LIMIT}}};$$  \hspace{1cm} (9)

where $V_{\text{RIPPLE}}$ is the maximum output ripple specification and $\text{I}_{\text{LIMIT}}$ is the LinkSwitch-TN current limit. The capacitor ESR value should be specified approximately at the switching frequency of 66 kHz.

Capacitor values above 100 $\mu F$ are not recommended as they can prevent the output voltage from reaching regulation during the 50 ms period prior to auto-restart. If more capacitance is required, then a soft-start capacitor should be added (see Other Information section).

**Step 8. Select the Feedback Resistors**

The values of $R_{FB}$ and $R_{\text{BIAS}}$ are selected such that, at the regulated output voltage, the voltage on the FEEDBACK pin ($V_{\text{FB}}$) is 1.65 V. This voltage is specified for a FEEDBACK pin current ($i_{\text{FB}}$) of 49 $\mu A$.

Let the value of $R_{\text{BIAS}} = 2 \text{ k}\Omega$; this biases the feedback network at a current of $-0.8 \text{ mA}$. Hence the value of $R_{\text{FB}}$ is given by

$$R_{\text{FB}} = \frac{V_o - V_{\text{FB}}}{\frac{V_o - V_{\text{FB}}}{R_{\text{BIAS}}} + i_{\text{FB}}} = \frac{(V_o - V_{\text{FB}}) \times R_{\text{BIAS}}}{V_o + (i_{\text{FB}} \times R_{\text{BIAS}})} = \frac{(V_o - 1.65 \text{ V}) \times 2 \text{ k}\Omega}{1.748 \text{ V}}$$  \hspace{1cm} (10)

**Step 9. Select the Feedback Diode and Capacitor**

For the feedback capacitor, use a 10 $\mu F$ general purpose electrolytic capacitor with a voltage rating $\geq 1.25 \times V_o^\prime$. For the feedback diode, use a glass passivated 1N4005GP or 1N4937GP device with a voltage rating of $\geq 1.25 \times V_{\text{MAX}}$.

**Step 10. Select Bypass Capacitor**

Use 0.1 $\mu F$, 50 V ceramic capacitor.

**Step 11. Select Pre-Load Resistor**

For direct feedback designs, if the minimum load <3 mA, then calculate $R_{PL} = V_o / 3$ mA.

**Other information**

**Start-Up Into Non-Resistive Loads**

If the total system capacitance is >100 $\mu F$ or the output voltage is >12 V, then during start-up the output may fail to reach regulation within 50 ms, triggering auto-restart operation. This may also be true when the load is not resistive, for example, the output is supplying a motor or fan. This is not applicable for the LNK302 as it does not have the auto-restart function.

To increase the start-up time, a soft-start capacitor can be added across the feedback resistor, as shown in Figure 3. The value of this soft-start capacitor is typically in the range of 0.47 $\mu F$ to 47 $\mu F$ with a voltage rating of $1.25 \times V_o^\prime$. Figure 4 shows the effect of $C_{\text{SS}}$ used on a 12 V, 150 mA design driving a motor load.

**Generating Negative and Positive Outputs**

In appliance applications there is often a requirement to generate both an AC line referenced positive and negative output. This can be accomplished using the circuit in Figure 5. The two Zener diodes have a voltage rating close to the required output voltage for each rail and ensure that regulation is maintained when one rail is lightly and the other heavily loaded. The LinkSwitch-TN circuit is designed as if it were a single output voltage with an output current equal to the sum of both outputs. The magnitude sum of the output voltages in this example being 12 V.
Constant Current Circuit Configuration (LED Driver)

The circuit shown in Figure 6 is ideal for driving constant current loads such as LEDs. It uses the tight tolerance and temperature stable FEEDBACK pin of LinkSwitch-TN as the reference to provide an accurate output current.

To generate a constant current output, the average output current is converted to a voltage by resistor RSENSE and capacitor CSENSE and fed into the FEEDBACK pin via RFB and RB.

With the values of RB and RFB as shown, the value of RSENSE should be chosen to generate a voltage drop of 2 V at the required output current. Capacitor CSENSE filters the voltage across RSENSE, which is modulated by inductor ripple current. The value of CSENSE should be large enough to minimize the ripple voltage, especially in MDCM designs. A value of CSENSE is selected such that the time constant (t) of RSENSE and CSENSE is greater than 20 times that of the switching period (15 µs). The peak voltage seen by CSENSE is equal to RSENSE × ILIMIT(MAX).

The output capacitor is optional; however with no output capacitor the load will see the full peak current (ILIMIT) of the selected LinkSwitch-TN. Increase the value of CO (typically in the range of 100 nF to 10 µF) to reduce the peak current to an acceptable level for the load.
If the load is disconnected, feedback is lost and the large output voltage which results may cause circuit failure. To prevent this, a second voltage control loop, DFB and VRFB, can be added as shown in Figure 6. This also requires that $C_O$ is fitted. The voltage of the Zener is selected as the next standard value above the maximum voltage across the LED string when it is in constant current operation.

The same design equations / design spreadsheet can be used as for a standard buck-boost design, with the following additional considerations.

1. $V_O = \text{LED } V_F \times \text{Number of LEDs per string}$.
2. $I_O = \text{LED } I_F \times \text{Number of strings}$.
3. Lower efficiency estimate due to $R_{\text{SENSE}}$ losses (enter $R_{\text{SENSE}}$ into design spreadsheet as inductor resistance).
4. Set $R_{\text{BASE}} = 2 \, \text{k}\Omega$ and $R_{\text{FB}} = 300 \, \Omega$.
5. $R_{\text{SENSE}} = 2/IO$.
6. $C_{\text{SENSE}} = 20 \times (15 \, \mu\text{s/R}_{\text{SENSE}})$.
7. Select $C_O$ based on acceptable output ripple current through the load.
8. If the load can be disconnected or for additional fault protection, add voltage feedback components DFB and VRFB, in addition to $C_O$.

**Thermal Environment**

To ensure good thermal performance, the SOURCE pin temperature should be maintained below 100 °C, by providing adequate heat sinking.

For applications with high ambient temperature (>50 °C), it is recommended to build and test the power supply at the maximum operating ambient temperature and ensure that there is adequate thermal margin. The figures for maximum output current provided in the data sheet correspond to an ambient temperature of 50 °C and may need to be thermally derated.

**Recommended Layout Considerations**

Traces carrying high currents should be as short in length and thick in width as possible. These are the traces which connect the input capacitor, LinkSwitch-TN, inductor, freewheeling diode, and the output capacitor.

Most off-the-shelf inductors are drum core inductors or dog-bone inductors. These inductors do not have a good closed magnetic path, and are a source of significant magnetic coupling. They are a source of differential mode noise and, for this reason, they should be placed as far away as possible from the AC input lines.

**Appendix A**

**Calculations for Inductor Value for Buck and Buck-Boost Topologies**

There is a minimum value of inductance that is required to deliver the specified output power, regardless of line voltage and operating mode.
The average current through the inductor over one switching cycle is equal to the output current \( I_O \). This current can be expressed as

\[
I_O = \frac{1}{T_{SW\_MIN}} \left( \frac{1}{2} \times (I_{LIMIT\_MIN} + I_{INITIAL}) \times t_{ON} + \frac{1}{2} \times (I_{LIMIT\_MIN} + I_{INITIAL}) \times t_{OFF} + 0 \times t_{IDLE} \right)
\]  
(A4)

where

\[
I_O = \text{Output current.}
\]

\[
T_{SW\_MIN} = \text{The switching interval corresponding to minimum switching frequency } F_{S\_MIN}.
\]

Substituting for \( t_{ON} \) and \( t_{OFF} \) from equations (A1) and (A2) we have

\[
I_O = \frac{1}{T_{SW\_MAX}} \left( \frac{1}{2} \times (I_{LIMIT\_MIN} + I_{INITIAL}) \frac{I_{RIPPLE}}{V_{MIN}} \times L_{MIN} \times F_{S\_MIN} \times (V_{MIN} - V_{DS}) \right)
\]

(A5)

\[
I_{L_MIN} = \frac{2 \times (V_O - I_O) \times (V_{MIN} - V_{DS} - V_O) \times (I_{LIMIT\_MIN}^2 - I_{INITIAL}^2) \times F_{S\_MIN} \times (V_{MIN} - V_{DS})}{(I_{LIMIT\_MIN} - I_{INITIAL})^2}
\]  
(A6)

For output voltages greater than 20 V, use \( V_{MAX} \) for calculation of \( L_{MIN} \) (Equation A6). For output voltages less than 20 V, use \( V_{MIN} \) for calculation of \( L_{MIN} \) to compensate for current limit delay time overshoot.

This however does not account for the losses within the inductor (resistance of winding and core losses) and the freewheeling diode, which will limit the maximum power delivering capability and thus reduce the maximum output current. The minimum inductance must compensate for these losses in order to deliver specified full load power. An estimate of these losses can be made by estimating the total losses in the power supply, and then allocating part of these losses to the inductor and diode. This is done by the loss factor \( K_{LOSS} \) which increases the size of the inductor accordingly.

Furthermore, typical inductors for this type of application are bobbin core or dog bone chokes. The specified current rating refer to a temperature rise of 20 °C or 40 °C and to an inductance drop of 10%. We must incorporate an inductance tolerance factor \( K_{L\_TOL} \) within the expression for minimum inductance, to account for this manufacturing tolerance. The typical inductance value thus can be expressed as

\[
L_{TYP} = \frac{2 \times K_{L\_TOL} \times \left( \frac{V_O \times I_o}{K_{LOSS}} \right) \times (V_{MIN} - V_{DS} - V_O) \times (I_{LIMIT\_MIN}^2 - I_{INITIAL}^2) \times F_{S\_MIN} \times (V_{MIN} - V_{DS})}{(I_{LIMIT\_MIN}^2 - I_{INITIAL}^2) \times F_{S\_MIN} \times (V_{MIN} - V_{DS})}
\]  
(A7)

where

\[
K_{LOSS} = \text{a loss factor, which accounts for the off-state total losses of the inductor.}
\]

\[
K_{L\_TOL} = \text{the inductor tolerance factor and can be between 1.1 and 1.2. A typical value is 1.15.}
\]

With this typical inductance we can express maximum output power as

\[
P_{O\_MAX} = \frac{1}{2} \times \left( \frac{V_O}{K_{LOSS}} \right) \times (I_{LIMIT\_MIN}^2 - I_{INITIAL}^2) \times F_{S\_MIN} \times \frac{V_{MIN} - V_{DS} - V_O}{V_{MIN} - V_{DS}}
\]  
(A8)

Similarly for buck-boost topology the expressions for \( L_{TYP} \) and \( P_{O\_MAX} \) are

\[
L_{TYP} = \frac{2 \times K_{L\_TOL} \times \left( \frac{V_O \times I_o}{K_{LOSS}} \right) \times (I_{LIMIT\_MIN}^2 - I_{INITIAL}^2) \times F_{S\_MIN}}{(I_{LIMIT\_MIN}^2 - I_{INITIAL}^2) \times K_{LOSS} \times F_{S\_MIN}}
\]

(A9)

\[
P_{O\_MAX} = \frac{1}{2} \times L_{TYP} \times (I_{LIMIT\_MIN}^2 - I_{INITIAL}^2)
\]

(A10)

**Average Switching Frequency**

Since LinkSwitch-TN uses an on-off type of control, the frequency of switching is non-uniform due to cycle skipping. We can average this switching frequency by substituting the maximum power as the output power in Equation A8. Simplifying, we have

\[
F_{S\_AVG} = \frac{2 \times V_O \times I_O \times K_{L\_TOL} \times \left( \frac{V_O}{K_{LOSS}} \right) \times (I_{LIMIT\_MIN}^2 - I_{INITIAL}^2) \times F_{S\_MIN} \times (V_{MIN} - V_{DS} - V_O)}{L \times (I_{LIMIT\_MIN}^2 - I_{INITIAL}^2) \times K_{LOSS}}
\]  
(A11)

Similarly for buck-boost converter, simplifying Equation A9 we have

\[
F_{S\_AVG} = \frac{2 \times V_O \times I_O \times \left( \frac{V_O}{K_{LOSS}} \right) \times \left( \frac{V_O}{K_{LOSS}} \right) \times K_{L\_TOL} \times K_{LOSS}}{L \times (I_{LIMIT\_MIN}^2 - I_{INITIAL}^2) \times K_{LOSS}}
\]  
(A12)

**Calculation of RMS Currents**

The RMS current value through the inductor is mainly required to ensure that the inductor is appropriately sized and will not overheat. Also, RMS currents through the LinkSwitch-TN and freewheeling diode are required to estimate losses in the power supply.

Assuming CCM operation, the initial current in the inductor in steady state is given by

\[
I_{INITIAL} = I_{LIMIT\_MIN} - \frac{V_O}{L} \times t_{OFF}
\]  
(A13)

For DCM operation this initial current will be zero.
The current through the LinkSwitch-TN as a function of time is given by

\[ i_{SW} (t) = I_{INITIAL} + \frac{V_{MIN} - V_{DS} - V_{O}}{L} \times t, 0 < t \leq t_{ON} \]

\[ i_{SW} (t) = 0, t_{ON} < t \leq t_{ON} \]

(A14)

The current through the freewheeling diode as a function of time is given by

\[ i_{D} (t) = I_{LIMIT\_MIN} - \frac{V_{O}}{L} \times t, 0 < t \leq t_{SW} \]

\[ i_{D} (t) = 0, I_{LIMIT\_MIN} - \frac{V_{O}}{L} \times t < 0 \]

(A15)

And the current through the inductor as a function of time is given by

\[ i_{L} (t) = i_{SW} (t) + i_{D} (t) \]

(A17)

From the definition of RMS currents we can express the RMS currents through the switch, freewheeling diode and inductor as follows

\[ i_{SW\_RMS} = \sqrt{\frac{1}{T_{AVG}} \int_{0}^{t_{ON}} (i_{SW} (t))^2 \times dt} \]

(A18)

\[ i_{D\_RMS} = \sqrt{\frac{1}{T_{AVG}} \int_{0}^{t_{SW}} (i_{D} (t))^2 \times dt} \]

(A19)

\[ i_{L\_RMS} = \sqrt{\frac{1}{T_{AVG}} \int_{0}^{T_{SW}} (i_{SW} (t) + i_{D} (t))^2 \times dt} \]

(A20)

Since the switch and freewheeling diode currents fall to zero during the turn off and turn on intervals respectively, the RMS inductor current is simplified to

\[ i_{L\_RMS} = \sqrt{i_{SW\_RMS}^2 + i_{D\_RMS}^2} \]

(A21)

Table A1 lists the design equations for important parameters using the buck and buck-boost topologies.

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Buck</th>
<th>Buck-Boost</th>
</tr>
</thead>
<tbody>
<tr>
<td>(L_{TYP})</td>
<td>(L_{TYP} = 2 \times K_{L} \times \left( V_{O} \times I_{D} \right) \times \left( V_{MIN} - V_{DS} - V_{O} \right) ) ((I_{LIMIT_MIN} - I_{INITIAL}) \times F_{SM_MIN} \times (V_{MIN} - V_{DS}))</td>
<td>(L_{TYP} = 2 \times K_{L} \times \left( V_{O} \times I_{D} \right) \times \left( I_{LIMIT_MIN} - I_{INITIAL} \right) \times F_{SM_MIN} \times K_{L_LOSS} )</td>
</tr>
<tr>
<td>(F_{AVG})</td>
<td>(F_{AVG} = 2 \times V_{O} \times I_{D} \times K_{L} \times \left( V_{MIN} - V_{DS} - V_{O} \right) ) ((I_{LIMIT_MIN}^2 - I_{INITIAL}^2) \times F_{SM_MIN} \times (V_{MIN} - V_{DS}))</td>
<td>(F_{AVG} = 2 \times V_{O} \times I_{D} \times K_{L} \times \left( I_{LIMIT_MIN}^2 - I_{INITIAL}^2 \right) \times F_{SM_MIN} \times K_{L_LOSS} )</td>
</tr>
<tr>
<td>(i_{SW} (t))</td>
<td>(i_{SW} (t) = I_{INIT} + \frac{V_{MIN} - V_{DS} - V_{O}}{L} \times t, t_{ON} \leq t \leq t_{ON} )</td>
<td>(i_{SW} (t) = I_{INIT} + \frac{V_{MIN} - V_{DS}}{L} \times t, t_{ON} \leq t \leq t_{ON} )</td>
</tr>
<tr>
<td>(i_{D} (t))</td>
<td>(i_{D} (t) = 0, t_{ON} &lt; t \leq t_{ON} )</td>
<td>(i_{D} (t) = 0, t_{ON} &lt; t \leq t_{ON} )</td>
</tr>
<tr>
<td>(i_{L} (t))</td>
<td>(i_{L} (t) = i_{SW} (t) + i_{D} (t) )</td>
<td>(i_{L} (t) = i_{SW} (t) + i_{D} (t) )</td>
</tr>
<tr>
<td>Max Drain Voltage</td>
<td>(V_{MAX} )</td>
<td>(V_{MAX} + V_{O} )</td>
</tr>
</tbody>
</table>

Table A1. Circuit Characteristics for Buck and Buck-Boost Topologies.
<table>
<thead>
<tr>
<th>Revision</th>
<th>Notes</th>
<th>Date</th>
</tr>
</thead>
<tbody>
<tr>
<td>A</td>
<td>Initial Release</td>
<td>01/04</td>
</tr>
<tr>
<td>B</td>
<td>Corrected Tables 3 and 4.</td>
<td>04/04</td>
</tr>
<tr>
<td>C</td>
<td>Added LNK302.</td>
<td>07/04</td>
</tr>
<tr>
<td>D</td>
<td>Added supplementary information to Tables 4 and 5.</td>
<td>12/04</td>
</tr>
<tr>
<td>E</td>
<td>Corrected equation 2.</td>
<td>05/05</td>
</tr>
<tr>
<td>F</td>
<td>Updated Key Features column in Table 1.</td>
<td>04/09</td>
</tr>
<tr>
<td>F</td>
<td>Fixed errors in Figures 1(a), 1(b) and 7.</td>
<td>03/14</td>
</tr>
</tbody>
</table>
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Power Integrations Worldwide Sales Support Locations

World Headquarters
5245 Hellyer Avenue
San Jose, CA 95138, USA.
Main: +1-408-414-9200
Customer Service:
Phone: +1-408-414-9665
Fax: +1-408-414-9765
e-mail: usasales@powerint.com

China (Shanghai)
Rm 2410, Charity Plaza, No. 88 North Caixi Road
Shanghai, PRC  200030
Phone: +86-21-6354-6323
Fax: +86-21-6354-6325
e-mail: chinasales@powerint.com

China (Shenzhen)
3rd Floor, Block A, Zhongtou International Business Center, No. 1061, Xiang Mei Rd, FuTian District, Shenzhen, China, 518040
Phone: +86-755-8379-3243
Fax: +86-755-8379-5828
e-mail: chinasales@powerint.com

Germany
Lindwurmstrasse 114
80337 Munich
Germany
Phone: +49-89-552-39110
Fax: +49-89-552-39200
e-mail: eurosales@powerint.com

India
#1, 14th Main Road
Vasanthanagar
Bangalore-560052 India
Phone: +91-80-4113-8020
Fax: +91-80-4113-8023
e-mail: indiasales@powerint.com

Italy
Via Milanesse 20, 3rd. Fl.
20099 Sesto San Giovanni (MI)
Italy
Phone: +39-024-550-8701
Fax: +39-028-928-6009
e-mail: eurosales@powerint.com

Japan
Kosei Dai-3 Bldg.
2-12-11, Shin-Yokohama,
Kohoku-ku
Yokohama-shi Kanagawan
222-0033 Japan
Phone: +81-45-471-1021
Fax: +81-45-471-3717
e-mail: japansales@powerint.com

Korea
RM 602, 6FL
Korea City Air Terminal B/D, 159-6
Samsung-Dong, Kangnam-Gu,
Seoul, 135-728, Korea
Phone: +82-2-2016-6610
Fax: +82-2-2016-6630
e-mail: koreasales@powerint.com

Singapore
51 Newton Road
#19-01/05 Goldhill Plaza
Singapore, 308900
Phone: +65-6358-2160
Fax: +65-6358-2015
e-mail: singaporesales@powerint.com

Taiwan
5F, No. 318, Nei Hu Rd., Sec. 1
Nei Hu Dist.
Taipei 11493, Taiwan R.O.C.
Phone: +886-2-2659-4570
Fax: +886-2-2659-4550
e-mail: taiwansales@powerint.com

Europe HQ
1st Floor, St. James’s House
East Street, Farnham
Surrey GU9 7TJ
United Kingdom
Phone: +44 (0) 1252-730-141
Fax: +44 (0) 1252-727-689
e-mail: eurosales@powerint.com

Applications Hotline
World Wide +1-408-414-9660
Applications Fax
World Wide +1-408-414-9760